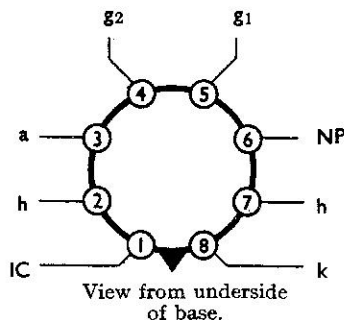


A beam tetrode with an absolute maximum anode dissipation rating of 30W. It is designed for use in the output stage of an a.f. amplifier, or as a series valve in a stabilized power supply.

The KT66 is a commercial version of the CV1075.

### BASE CONNECTIONS AND VALVE DIMENSIONS



Base: International Octal (B8-0)  
Bulb: Dome top tubular

Max. overall length : 135 mm  
Max. seated length : 121 mm  
Max. diameter : 53 mm

### HEATER

$V_h$	6.3	V
$I_h$	1.3 (approx)	A

### MAXIMUM RATINGS

	<i>Design Max.</i>	<i>Absolute Max.</i>	
$V_a$	500	550	V
$V_{g2}$	500	550	V
$-V_{g1}$	200	200	V
$I_k$	200	200	mA
$P_a$	25	30	W
$P_{g2}$	3.5	4.5	W
* $P_{a+g2}$	27	32	W
$V_{h-k}$	150	150	V
$T_{bulb}$	250	250	°C
$R_{g1-k}$ (cathode bias) :			
$P_{a+g2} < 27W$		1.0	MΩ
$P_{a+g2} > 27W$	500		kΩ
$R_{g1-k}$ (fixed bias) :			
$P_{a+g2} < 27W$	250		kΩ
$P_{a+g2} > 27W$	100		kΩ

\*Triode or ultra-linear operation.

### CAPACITANCES (Measured on a cold unscreened valve)

$C_{g1}$ —all, less a : 14.5 pF       $C_a$ —all, less  $g1$  : 10.0 pF       $C_{a-g1}$  : 1.1 pF

### CHARACTERISTICS

#### Tetrode Connection

$V_a$	250	V
$V_{g2}$	250	V
$-V_{g1}$	15	V
$g_m$	7	mA/V
$r_a$	22.5	kΩ

# KT66

## Triode Connection

$V_a$	250	V
$-V_{g1}$	15	V
$g_m$	7.3	mA/V
$r_a$	1.3	k $\Omega$

## TYPICAL OPERATION

### Triode Connection. Class A. Single Valve. Cathode Bias.

$V_{a,g2(b)}$	270	440	V
$V_{a,g2}$	250	400	V
$-V_{g1}$ (approx)	20	38	V
$v_{in(pk)}$	20	38	V
$R_k$	330	600	$\Omega$
$I_{a+g2(o)}$	60	63	mA
$P_{a+g2(o)}$	15	25	W
$R_L$	2.75	4.5	k $\Omega$
$P_{out}$	2.2	5.8	W
$D_{tot}$	6	7	%

### Triode Connection. Class AB1. Push-Pull. Cathode Bias.

$V_{a,g2(b)}$	270	440	V
$V_{a,g2}$	250	400	V
$-V_{g1}$ (approx)	19	38	V
$v_{in(g1-g1)(pk)}$	38	76	V
* $R_k$	2 x 345	2 x 615	$\Omega$
$I_{a+g2(o)}$	2 x 55	2 x 62	mA
$P_{a+g2(o)}$	2 x 14	2 x 25	W
$R_L(a-a)$	2.5	4.0	k $\Omega$
$P_{out}$	4.5	14.5	W
$D_{tot}$	2.0	3.5	%
†IM	3.0	3.0	%
$z_{out}$	3.5	3.5	k $\Omega$

\*It is essential to use two separate cathode bias resistors.

†Intermodulation distortion ; measured using two input signals at 50 and 6000c/s (ratio of amplitudes 4:1).

### Tetrode Connection. Class AB1. Push-Pull. Cathode Bias.

$V_a(b)(o)$	450	V
$V_a(b)(max\ sig)$	425	V
$V_a(o)$	415	V
$V_a(max\ sig)$	390	V
$V_{g2(o)}$	300	V
$V_{g2(max\ sig)}$	275	V
$-V_{g1}$ (approx)	27	V
$I_a(o)$	2 x 52	mA
$I_a(max\ sig)$	2 x 62	mA
$I_{g2(o)}$	2 x 2.5	mA
$I_{g2(max\ sig)}$	2 x 9	mA
$P_a(o)$	2 x 21	W
$P_a(max\ sig)$	2 x 9.0	W
$P_{g2(o)}$	2 x 0.75	W
$P_{g2(max\ sig)}$	2 x 2.5	W
* $R_k$	2 x 500	$\Omega$
$R_L(a-a)$	8	k $\Omega$
$v_{in(g1-g1)(pk)}$	70	V
$P_{out}$	30	W
$D_{tot}$	6	%

\*It is essential to use two separate cathode bias resistors.

### Ultra-linear Connection. Push-Pull. 40% Taps. Class AB1. Cathode Bias.

$V_a(b)$	450	V
$V_{a,g2(o)}$	425	V
$V_{a,g2(max\ sig)}$	400	V
$I_{a+g2(o)}$	2 x 62.5	mA
$I_{a+g2(max\ sig)}$	2 x 72.5	mA

$P_{a+g2(o)}$	$2 \times 26.5$	W
$P_{a+g2(max sig)}$	$2 \times 13.0$	W
* $R_k$	$2 \times 560$	$\Omega$
$-V_g$ (approx)	35	V
$P_{out}$	32	W
$R_{L(a-a)}$	7	k $\Omega$
$z_{out}$	9	k $\Omega$
$D_{tot}$	2	%
$\uparrow IM$	4	%

\*It is essential to use two separate cathode bias resistors.

$\uparrow$ Intermodulation distortion ; measured using two input signals at 50 and 6000c/s (ratio of amplitudes 4:1).

### Ultra-linear Connection. Class AB1. Push-Pull. 40% Taps. Fixed Bias.

$V_{a,g2(o)}$	525	V
$V_{a,g2(max sig)}$	500	V
$I_{a+g2(o)}$	$2 \times 35$	mA
$I_{a+g2(max sig)}$	$2 \times 80$	mA
$P_{a+g2(o)}$	$2 \times 18$	W
$P_{a+g2(max sig)}$	$2 \times 15$	W
* $-V_{g1}$ (approx)	67	V
$R_{L(a-a)}$	8	k $\Omega$
$v_{in(g1-g1)(pk)}$	127	V
$P_{out}$	50	W
$D_{tot}$	3	%
$\uparrow IM$	15	%
$z_{out}$	10	k $\Omega$

\*A negative bias range of  $\pm 25\%$  of this value should be available for each valve.

$\uparrow$ Intermodulation distortion ; measured using two input signals at 50 and 6000c/s (ratio of amplitudes 4:1).

### LIFE PERFORMANCE

The average life expectancy of the KT66 when operated at absolute maximum ratings (see page 1) is at least 8000 hours. At a reduced absolute rating of  $p_{a+g2}=21W$  a life of at least 10000 hours should be obtained. The environment must be a static one and the valve should be switched not more than 12 times in each 24 hours. Attention should also be paid to the recommendations of the British Standard Code of Practice CP1005 *The Use of Electronic Valves*.

A valve is considered to have reached the end of life when it is either inoperative or one or more of its characteristics have reached the following values:

$P_{out}$	50% of initial value	
* $g_m$	<5.5	mA/V
*Measured at:		
$V_a$	250	V
$V_{g2}$	250	V
$I_a$	85	mA

### INSTALLATION

The valve may be mounted in any position but when horizontal it should be orientated as shown in fig. 1. No retaining device or external screening is normally necessary.

Adequate ventilation should be provided. A pair of valves working at maximum ratings should be mounted at not less than 3.5 in. (9 cm) between centres.

For the prevention of parasitic oscillation, a series resistor of 100—300 $\Omega$  should be connected close to the screen tag of the valve socket. When the valve is triode connected, this resistor should be connected between screen and anode. A control grid series resistor of 10-50k $\Omega$  is also recommended. In push-pull applications having a large change in anode current between the quiescent and full output conditions, an inductance input filter circuit of good regulation should be used. A badly regulated supply will cause a fall in power output and/or excessive quiescent anode dissipation.

# KT66

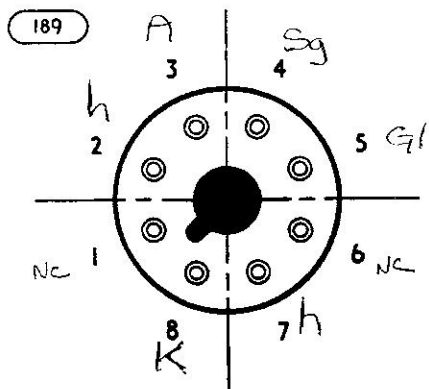


Fig. 1. Correct orientation of the valve socket for horizontally mounting the KT66.

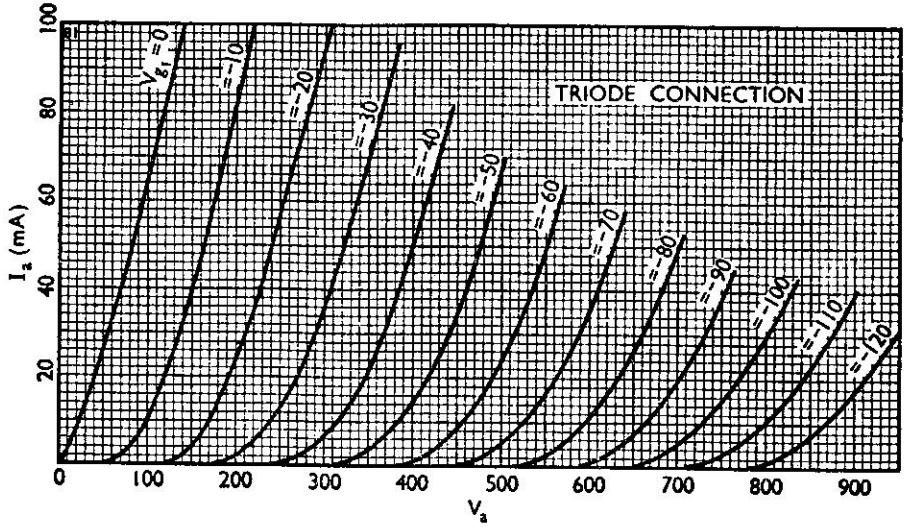


Fig. 2.

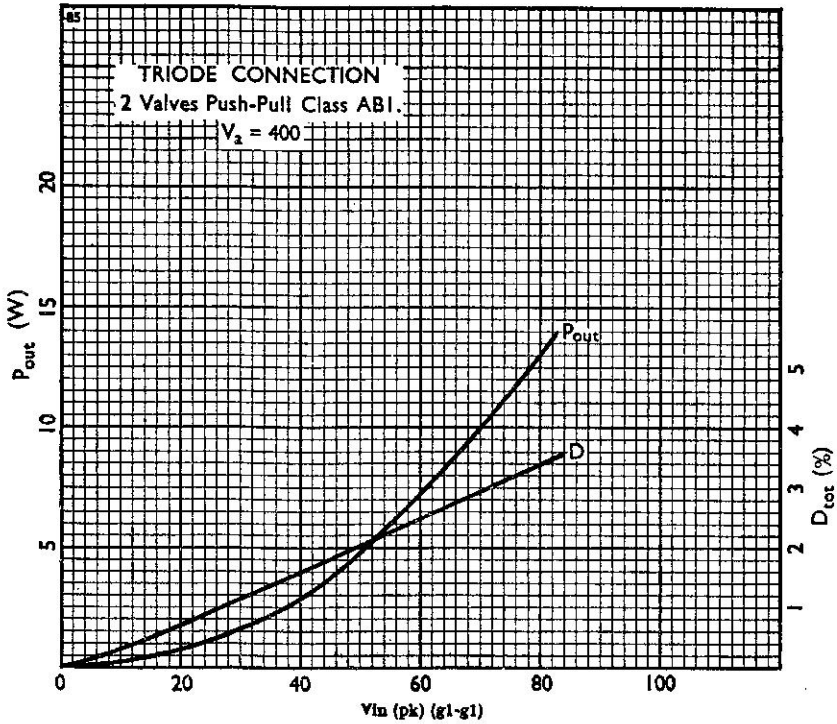


Fig. 3.

# KT66

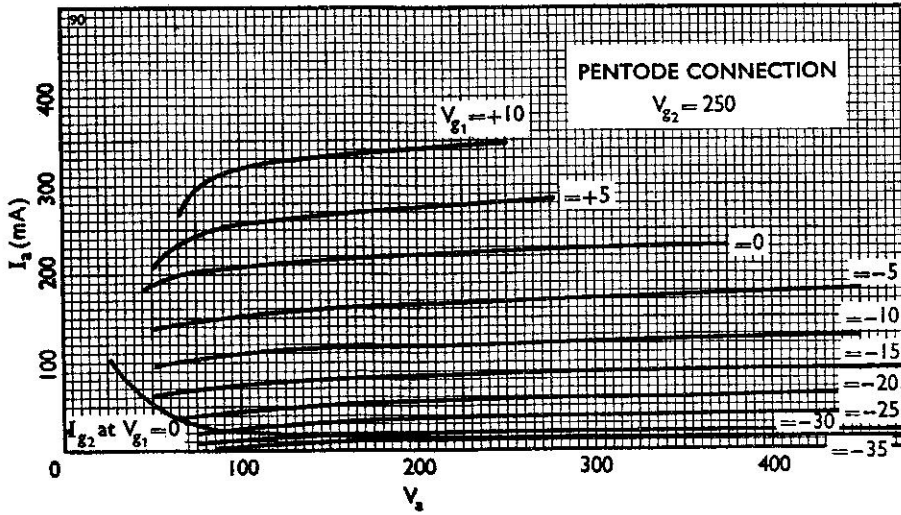


Fig. 4.

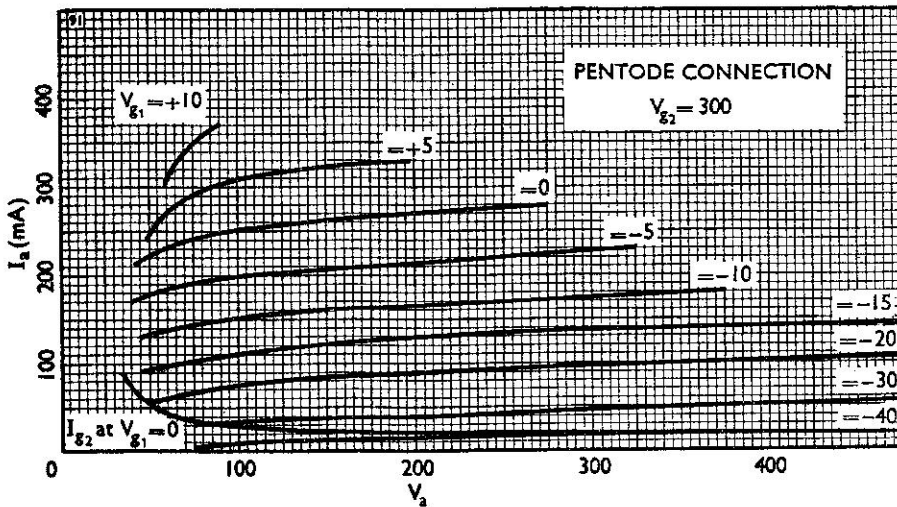


Fig. 5.

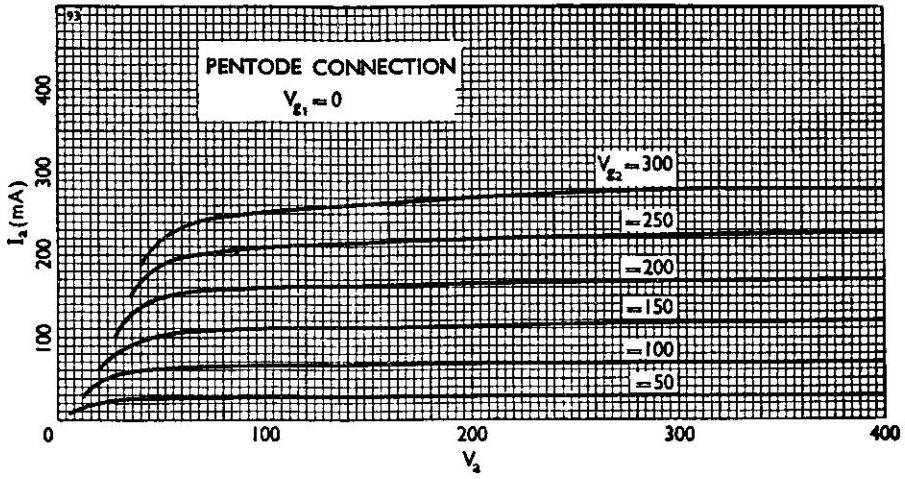


Fig. 6.

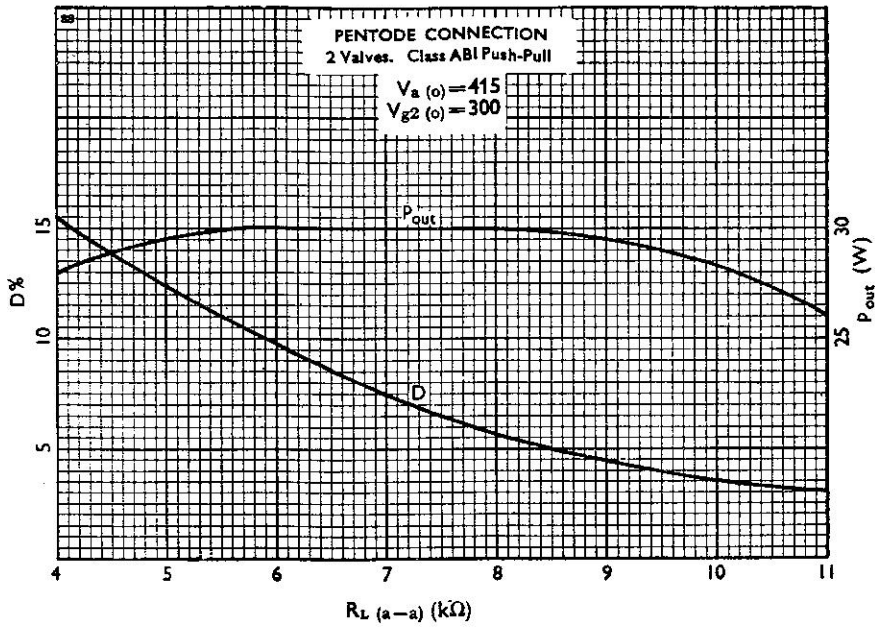


Fig. 7.

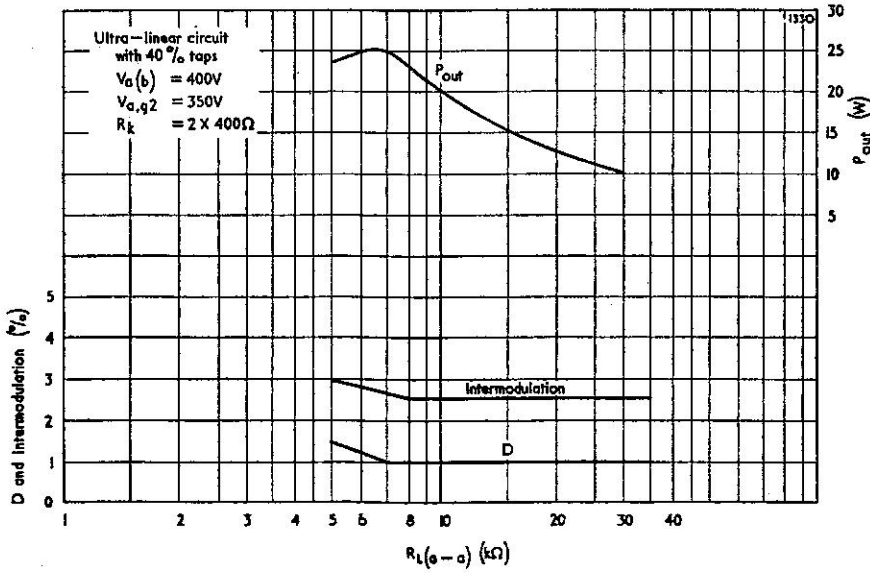


Fig. 8.

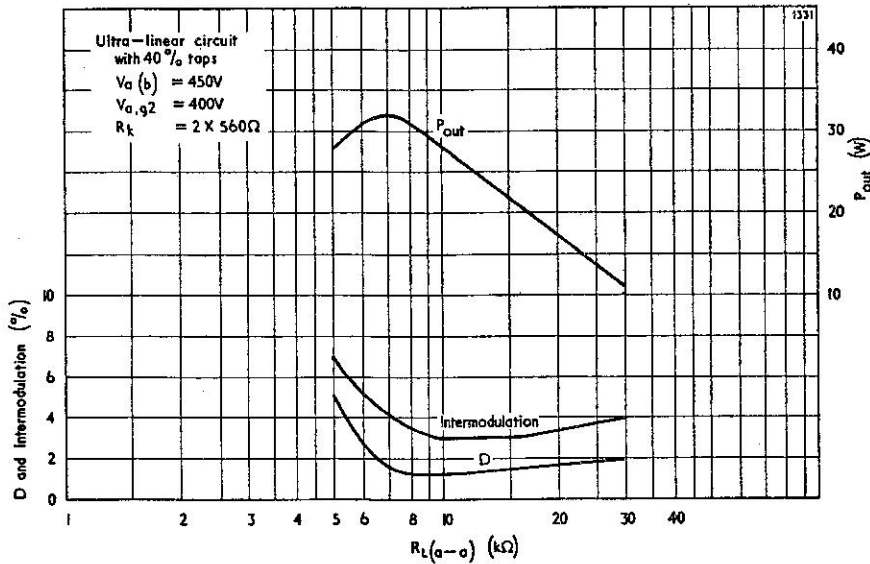


Fig. 9.

The above curves show power output, harmonic distortion and intermodulation plotted against load impedance. Ultra-linear operation at two values of  $V_a(b)$ .



This supplement contains comparisons of the performance of the KT66 under the three different operating conditions of triode, pentode and ultra linear connections. Design details of 30W and 50W ultra linear amplifiers are also given.

The data on normal triode or pentode operation of the KT66 is well-known and is not given here.\* In ultra linear operation, the screen grid of each KT66 is returned to a tapping point on the output transformer primary. These tapping points include 20% of the total turns of each half primary, counting from the centre. The voltage during the operating cycle is not held constant, as with pentode operation, nor does it take up the instantaneous anode voltage as in the triode condition. It combines the advantages of both systems in that the high power output of the pentode is still obtainable but with the low distortion of the triode arrangement.

Considerable publicity has been given to this arrangement in the British and American press and in general the claims made are substantiated.

### **CIRCUIT**

The circuit is shown in fig. 1. The two KT66 valves are preceded by a pair of B65 double triode valves, one of which is used as a self-balancing phase inverter and the other as a push-pull voltage amplifier. Full output is given for an input of about 150mV rms.

In ultra linear operation the KT66 valves have their screen grids returned to tapping points on each half primary. When measurements are made under triode conditions, each screen is connected to its anode, and for pentode operation, the screens are connected to the 450V line.

It has been found desirable to connect capacitors C13, C14 of 2000pF across part of the output transformer in the interests of stability. Screen grid and control grid resistors R15, R16, R17 and R18 are included for the same reason.

Independent cathode bias resistors R11, R12 of 560 $\Omega$  are used, a value satisfactory for all three classes of operation.

The small capacitors C5, C6 serve to neutralise stray capacitances in the phase inverter stage and ensure that a balanced output is obtained at the higher frequencies. Their value is not critical but they should be both the same.

In order to obtain the full advantages of the ultra linear circuit, an output transformer of high quality is required. That used in the design of this amplifier was made by Partridge Transformers Ltd., Ref. No. C1732. It has two equal secondaries in order to provide either a 4 $\Omega$  or 15 $\Omega$  output. Other details are :—

Leakage inductance : 15mH

Primary inductance : 80H

Ratio : 22:1

\*See the KT66 data sheet

## PERFORMANCE

The curves in figs. 2 and 3 show the performance of the three classes of operation at varying anode loads. Fig. 2 shows the ultra linear circuit at three different levels of distortion compared with the triode performance at full output. Fig. 3 shows the pentode condition together with a comparative triode curve.

It will be seen that the ultra linear circuit behaves quite differently from the pentode. With the latter, full output is obtainable with a distortion which varies between 4% and 6% according to anode load. Except at the lower load impedances, the output for 1% and 2% distortion is only a small proportion of the maximum output.

In the ultra linear arrangement, almost full output is obtained at 2% distortion and very little increase is obtained if this is permitted to rise to 3%. The output for 1% distortion is about 50% of the maximum.

It will be seen that, for most values of anode load impedance, the ultra linear circuit produces only one half the distortion of the triode for equivalent outputs and is capable also of giving double the output for the same order of distortion.

The output impedance of the ultra linear circuit is considerably lower than the pentode arrangement, though higher than the triode. Measurements made at 20W output with the optimum anode load of  $7k\Omega$  show that the ultra linear and pentode circuits have impedances of  $9k\Omega$  and  $35k\Omega$  respectively. A comparable measurement on the triode circuit gave  $3.5k\Omega$ . The ultra linear circuit has, therefore, an impedance similar to the anode-anode load impedance of  $7k\Omega$ , whereas the pentode impedance is very much higher. The ultra linear circuit can exert a considerable damping factor, a valuable asset if the load is a loudspeaker.

The frequency response of the complete amplifier of fig. 1 shows a loss of 1.5db at 20c/s and 25kc/s.

## OPERATING CONDITIONS

In all three classes of operation discussed, the anode and screen voltages were equal and maintained at 400 relative to the cathode. The KT66 is not normally used, as a pentode, with an equal anode and screen voltage of 400 due to the high screen current of 12mA per valve at maximum output. Under a sustained output the screen dissipation rating would be exceeded, although this method of operation is satisfactory for normal speech and music. Under these conditions, the current consumption is high but a saving is effected by the elimination of the stabiliser valve normally required in the pentode screen circuit. With the ultra linear circuit, the objection to the high current is removed since this does not exceed 7mA at maximum output. The screen current under the triode condition is, of course, lower still, at about 4mA per valve.

The data given in fig. 3 does not correspond with that previously published due to the use of a higher screen voltage. However, a closer comparison between the three operating conditions is obtained with constant voltages.

At full output, a voltage of 475 rms is present across the primary of the output transformer. The KT66 anodes therefore swing  $400 \pm 340V$ , i.e. 60 to 740V. The two screen grids have the same d.c. potential but the a.c. voltage is one-fifth of the anode swing. They therefore operate between 335 and 465V.

**COMPARISON OF OPERATING CONDITIONS**

	<i>Triode</i>	<i>Pentode*</i>	<i>Ultra Linear</i>	
V <sub>a</sub> (b)	450	450	450	V
V <sub>a</sub>	400	400	400	V
V <sub>g2</sub>	400	400*	400	V
I <sub>a+g2</sub>	125	125	125	mA
I <sub>g2</sub> (o)	5	5	5	mA
I <sub>a+g2</sub> (max sig)	135	155	145	mA
I <sub>g2</sub> (max sig)	8	24*	15	mA
R <sub>k</sub> (per valve)	560	560	560	Ω
V <sub>k</sub> (app)	36	36	36	V
P <sub>in</sub> (o)	50	50	50	W
P <sub>in</sub> (max sig)	54	62	58	W
P <sub>out</sub>	15	32	32	W
η	28	52	55	%
D (max sig)	2	≥6	2	%
R <sub>L(a-a)</sub>	6	7	7	kΩ
Z <sub>out</sub>	3.5	35	9	kΩ
V <sub>in(g1-g1)</sub> (rms)	52	42	56	V
Relative P <sub>out</sub> for given V <sub>in</sub>	{ ×1 0	×5 +7	×2.5 +4	db

\*Suitable for intermittent operation only, due to excessive screen dissipation at full output. When continuous full output is required, use the operating condition : V<sub>a</sub>=400, V<sub>g2</sub>=300.

**ADDITION OF NEGATIVE FEEDBACK**

Negative feedback may be added to the circuit of fig. 1 when an improved performance is required. It is suggested that 14db feedback is adequate for all normal purposes, although this may be increased if necessary. The application of 14db feedback will reduce the output impedance, distortion and overall sensitivity by a factor of five. This will provide an amplifier having the following characteristics :

- Input for full output : 600mV rms.
- Output impedance : 1.8kΩ
- Distortion : 0.5%
- Damping factor : 4

The method is shown in fig. 4, the feedback voltage being introduced into the cathode circuit of the first valve. The bias resistor R22 (shown as R2 in fig. 1) is connected in the cathode circuit of one triode only. A further bias resistor and capacitor, R23, C23, are provided and feedback is applied across R24 from the secondary of the output transformer via R25.

Since the basic sensitivity of the amplifier is approximately 120mV for full output, a feedback voltage of about 500mV is required for 14db negative feedback. The output voltage is 21.5 for Z<sub>o</sub>=15Ω and 11 for Z<sub>o</sub>=4Ω ; therefore, the two resistors R24, R25 are chosen so that 500mV will exist at their junction at full output.

Assuming that R24 has a value of 22Ω, the value of R25 is given by 225 √Z<sub>o</sub> and the nearest standard values may be used. For Z<sub>o</sub>=15 or 4Ω, resistors of 1kΩ or 470Ω are satisfactory.

# KT66 CIRCUIT SUPPLEMENT

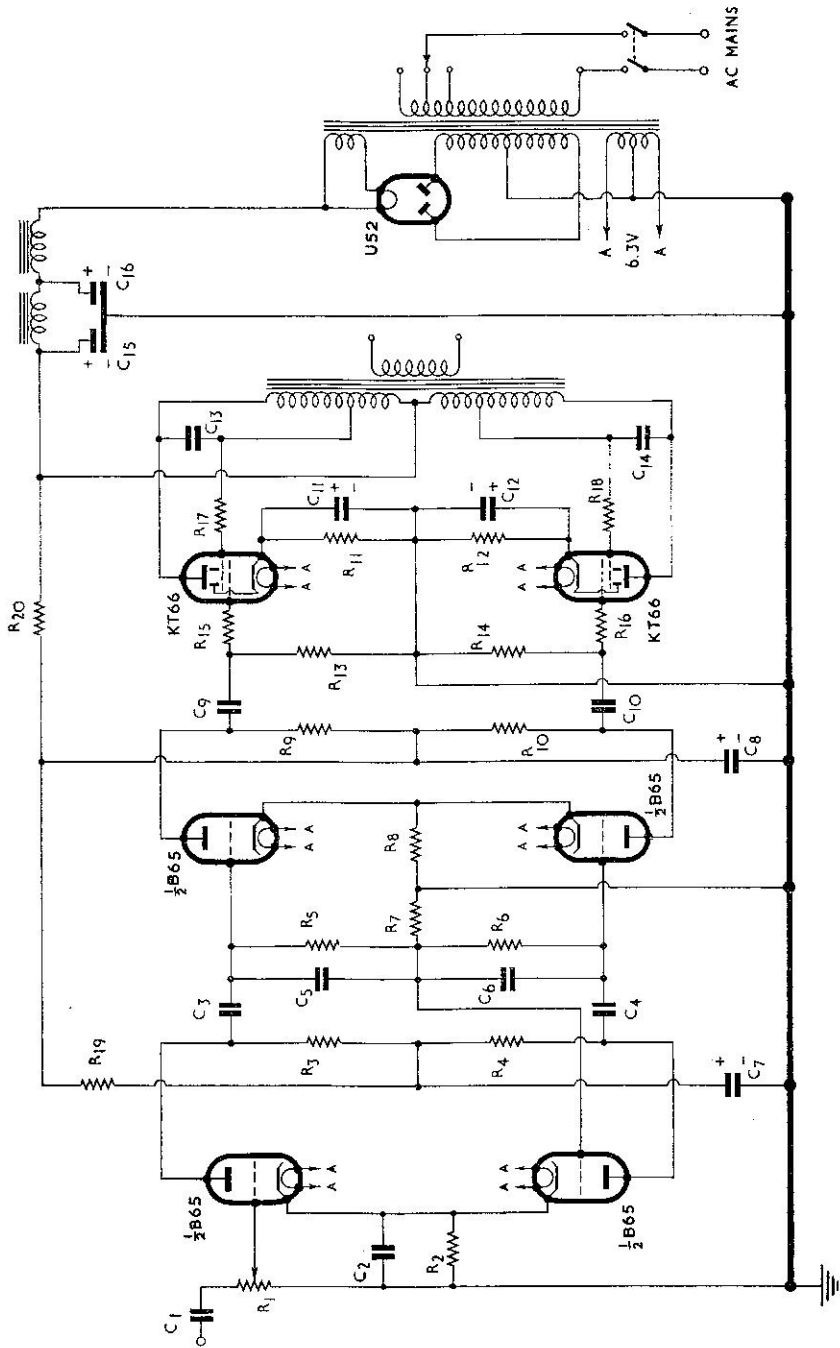


Fig. 1. A 30W ultra linear amplifier.  
Component values are given on pages 8 and 9.

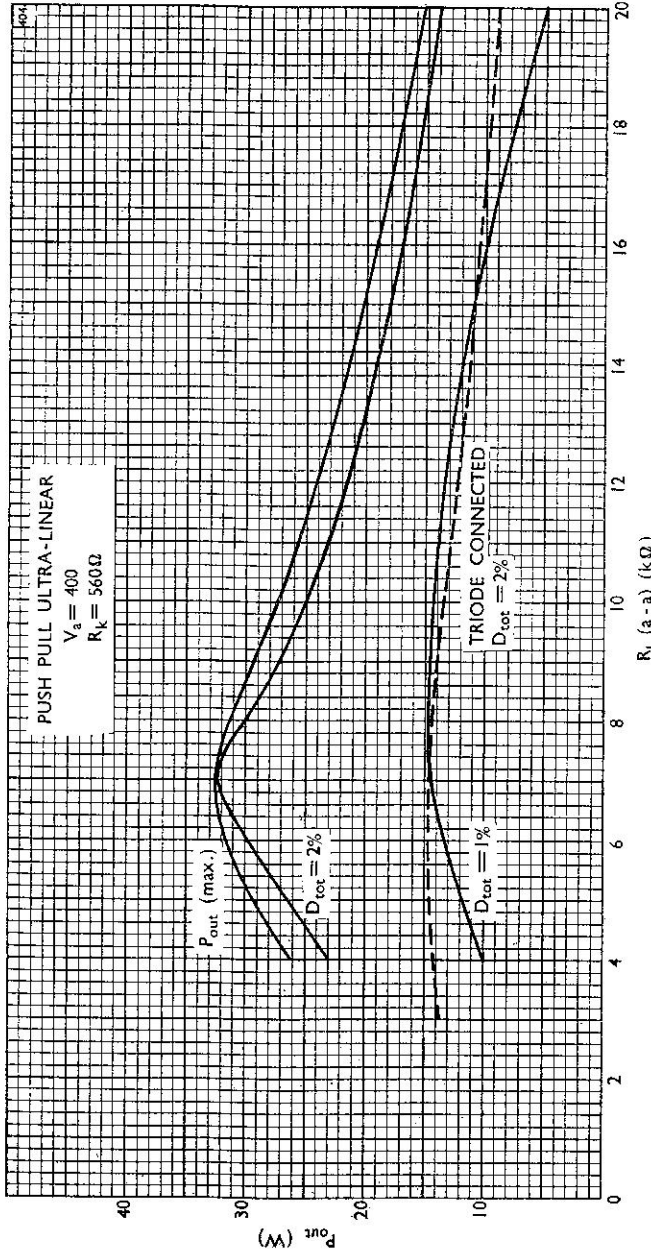


Fig. 2. A comparison of ultra linear with triode operation.

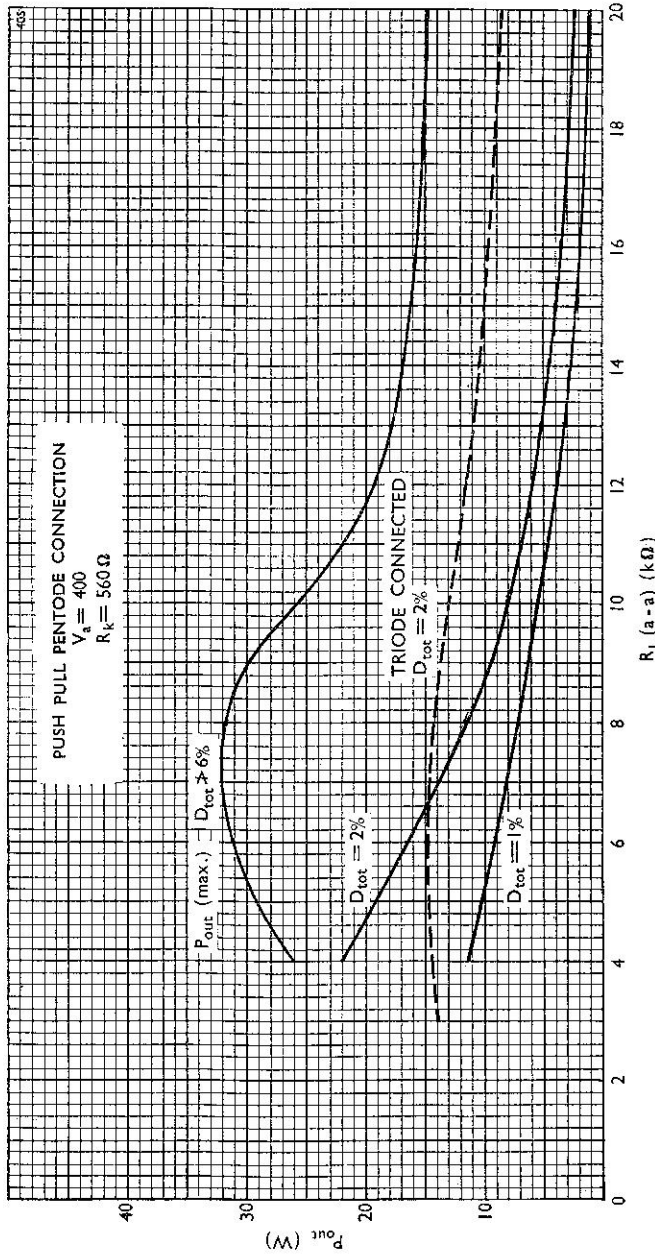


Fig. 3. A comparison of pentode with triode operation.

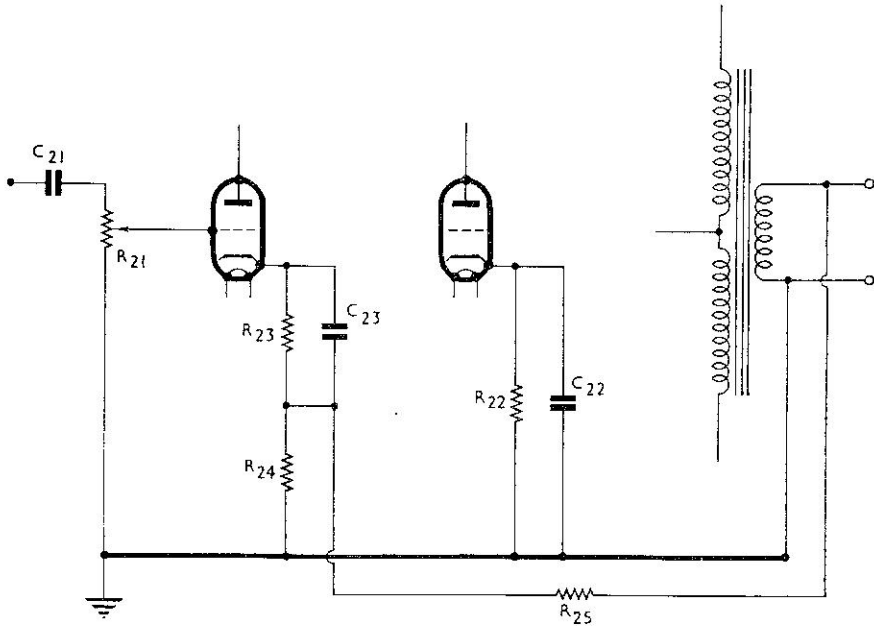


Fig. 4. The addition of negative feedback to the amplifier of fig. 1.  
See pages 8 and 9 for component values.

### A 50W ULTRA LINEAR AMPLIFIER

When the maximum output is required from a pair of KT66 valves they may be used with fixed bias in the ultra-linear circuit. The operating conditions are given below and the recommended circuit is shown in fig. 5.

Per Pair of Valves	Quiescent	Max. Signal	
$V_{a,g2}$	525	500	V
$I_{a+g2}$	70	160	mA
$V_{g1}$	-50/-65	-50/-65	V
$\dagger R_{L(a-a)}$	—	8	k $\Omega$
$P_{out}$	—	50	W
*D	—	2	%
$P_{a+g2}$ (per valve)	18	15	W
$z_{out}$	—	6	k $\Omega$
$V_{in(g1-g1)}$ (rms)	—	90	V
$V_{in}$ (to amplifier in fig. 5)	—	2.5	V

$\dagger$ An output transformer having a ratio of 6 : 1 would be suitable for 105V output, 225 $\Omega$ .

\*The distortion will vary from 1% to 3% with different valves. The performance is displayed graphically in figs. 7 and 8.

#### Circuit Notes.

The two KT66 valves are set to a similar quiescent current, which may be between 30 and 40mA, using the meter M and the meter shunts R46, R47. A negative bias voltage range of 50 to 65 is provided by the controls R53, R54. A quiescent current below 30mA will increase the distortion.

The bias voltage is derived from a U50 connected to the 600-0-600V transformer via the capacitors C42, C43. The resistors R55, R56, R57, R58, not only smooth the supply in conjunction with C44 but also reduce the voltage to the appropriate value. The resistors R52 to R58, associated with the bias supply, are generously rated to maintain a stable voltage.

R64 is adjusted, at about 90% of full output, to give equal cathode currents in the two output valves. It is capable of compensating for inequality of output from the driver stage and also for variations between the two output valves. When the two cathode currents are equal the distortion is at a minimum.

# KT66 CIRCUIT SUPPLEMENT

The anode supply is provided with an inductance filter L1, C31, C32. Due to the large variation in current with input signal the effective capacitance of C31, C32 has been made 80 $\mu$ F. The working voltage is excessive for a single electrolytic and C31, C32 are, therefore, connected in series to give a rated voltage of 900. This single section filter provides a ripple-free anode current. If a lower capacitance were used in place of C31, C32, an additional filter section would be required to reduce the ripple to a reasonable value, and the lower capacitance would be incapable of supplying the peak current required by a transient input signal.

At lower anode voltages the following results are obtainable. No circuit modifications are needed, the bias supply being a function of the anode voltage.

DC voltage	350	425	V
Quiescent current	25+25	30+30	mA
Max. signal current	55+55	65+65	mA
Power output	20	30	W
Anode to anode load	8	8	k $\Omega$

The value of the components C40, C41, C45 and R59 will depend to some extent on the output transformer. R59 and C45 are optional and are used to suppress ringing. The most satisfactory method of selecting the value of these four components is by the use of a square wave generator, but an audio oscillator extending to, say, 50kc/s may be used to detect a peak in the supersonic region. C40 and C41 may be unnecessary with some types of transformer.

With the transformer used, the values shown gave a fall in output of 3db at 18-20kc/s with a load resistance of 15 $\Omega$ .

## Protection Against Bias Failure.

In common with other amplifiers which derive the bias potential from a separate supply instead of a cathode resistor, the 50W amplifier is rendered inoperative should the bias supply fail. Furthermore, the KT66 anode current would rise to an excessive value. The U50 is run at a very low anode current, a few milliamperes, and will, of course, have a long life.

A simple device which permits the amplifier to function with cathode bias in case of failure of the bias supply is shown in fig. 6. A triode, which could be one half of a B65 substituted for the L63 in the first stage, is connected in series with a relay across the 500V supply. The grid is taken to the bias supply. Normally the anode current is cut off and the relay short-circuits the resistor R60 connected in the cathode circuit of the KT66 valves. Should the bias fail, the relay will be energised, the relay contacts will open and the bias resistor R60 will allow the amplifier to function at about half maximum output.

## COMPONENT VALUES

### RESISTORS

(0.25W, 20% unless otherwise shown)

R1	500k $\Omega$		
R2	750 $\Omega$		
R3	33k $\Omega$	1W	10%
R4	33k $\Omega$	1W	10%
R5	270k $\Omega$	} matched to 5%	
R6	270k $\Omega$		
R7	270k $\Omega$		10%
R8	750 $\Omega$		10%
R9	33k $\Omega$	1W	10%
R10	33k $\Omega$	1W	10%
R11	560 $\Omega$	5W w.w.	5%
R12	560 $\Omega$	5W w.w.	5%
R13	270k $\Omega$		10%
R14	270k $\Omega$		10%
R15	10k $\Omega$		
R16	10k $\Omega$		
R17	220 $\Omega$		
R18	220 $\Omega$		
R19	10k $\Omega$	0.5W	
R20	5.6k $\Omega$	1W	
R21	500k $\Omega$		
R22	750 $\Omega$		
R23	750 $\Omega$		



R24 } R25 }	sec p. 3		
R31	1M $\Omega$		
R32	33k $\Omega$	0.5W	} matched to 5%
R33	33k $\Omega$	0.5W	
R34	1.5k $\Omega$		
R35	1k $\Omega$		
R36	22k $\Omega$	0.5W	
R37	1M $\Omega$		
R38	1M $\Omega$		
R39	47k $\Omega$	1W	10%
R40	47k $\Omega$	1W	10%
R41	150k $\Omega$		10%
R42	150k $\Omega$		10%
R43	10k $\Omega$	1W	10%
R44	10k $\Omega$		
R45	10k $\Omega$		
R46 } R47 }	Meter shunts		
R48	10 $\Omega$		
R49	10 $\Omega$		
R50	100 $\Omega$		
R51	100k $\Omega$	1W	10%
R52 (see fig. 6)	100k $\Omega$	1W	10%
R53	22k $\Omega$	1W	10%
R54	20k $\Omega$	w.w.	
R55	20k $\Omega$	w.w.	
R56	220k $\Omega$	1W	10%
R57	220k $\Omega$	1W	10%
R58	220k $\Omega$	1W	10%
R59	220k $\Omega$	1W	10%
R60 (see fig. 6)	330 $\Omega$	5W w.w.	10%
R61 (see fig. 6)	6.6 k $\Omega$	0.5W	10%
R62	15k $\Omega$	0.5W	10%
R63	0.65 $\Omega$	5W	
R64	20k $\Omega$		

**CAPACITORS**

C1	0.01 $\mu$ F	350V	
C2	50 $\mu$ F	12V	Electrolytic
C3	0.1 $\mu$ F	500V	
C4	0.1 $\mu$ F	500V	
C5	100pF	250V	
C6	100pF	250V	
C7	8 $\mu$ F	450V	Electrolytic
C8	8 $\mu$ F	450V	Electrolytic
C9	0.02 $\mu$ F	500V	
C10	0.02 $\mu$ F	500V	
C11	50 $\mu$ F	50V	Electrolytic
C12	50 $\mu$ F	50V	Electrolytic
C13	2000pF	500V	
C14	2000pF	500V	
C15	8 $\mu$ F	450V	Electrolytic
C16	8 $\mu$ F	450V	Electrolytic
C21	0.01 $\mu$ F	350V	
C22	50 $\mu$ F	12V	Electrolytic
C23	50 $\mu$ F	12V	Electrolytic
C31	160 $\mu$ F	450V	Electrolytic
C32	160 $\mu$ F	450V	
C33	8 $\mu$ F	450V	
C34	8 $\mu$ F	450V	
C35	0.01 $\mu$ F	350V	
C36	0.01 $\mu$ F	500V	
C37	0.01 $\mu$ F	500V	
C38	0.05 $\mu$ F	750V	
C39	0.05 $\mu$ F	750V	
C40	0.001 $\mu$ F	300V AC	
C41	0.001 $\mu$ F	300V AC	
C42	0.025 $\mu$ F	600V AC	
C43	0.025 $\mu$ F	600V AC	
C44	4 $\mu$ F	200V	
C45	0.001 $\mu$ F	440V AC	

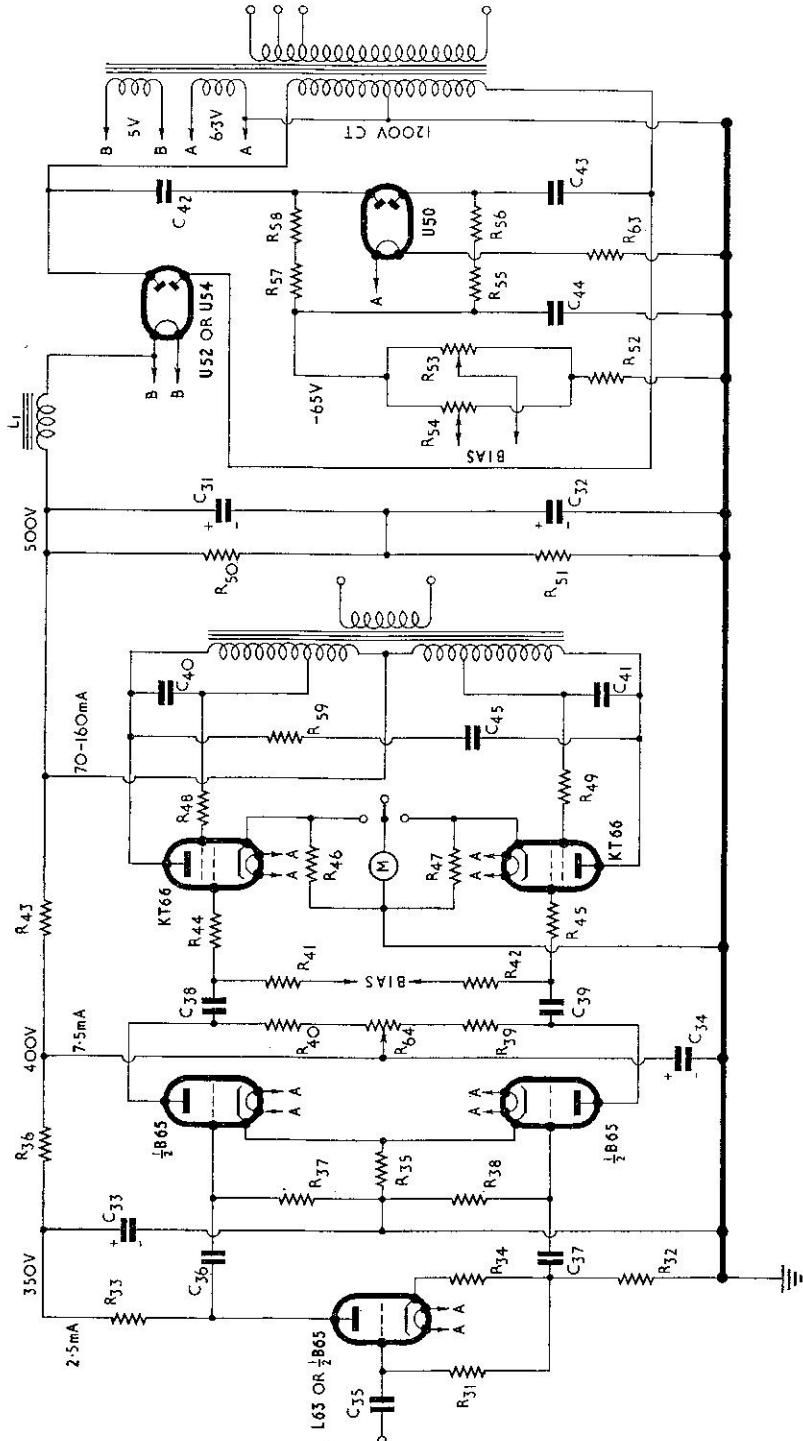


Fig. 5. A 60W ultra linear amplifier. See pages 8 and 9 for component values.

Fig. 6. This circuit may be added to the 50W amplifier to protect the KT66 valves in the event of bias failure. The resistor R60, normally short-circuited by the relay, provides an emergency cathode bias. R61 and R62 replace R52.

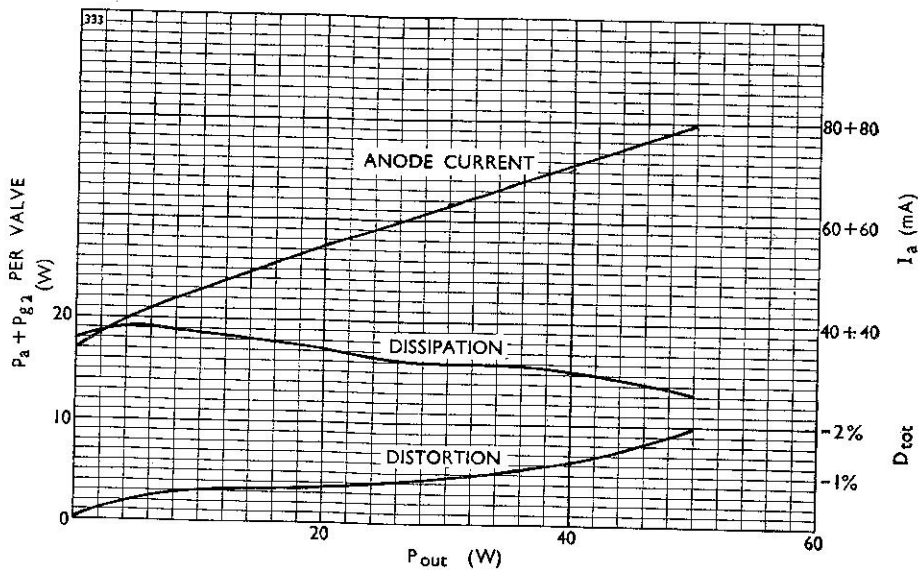
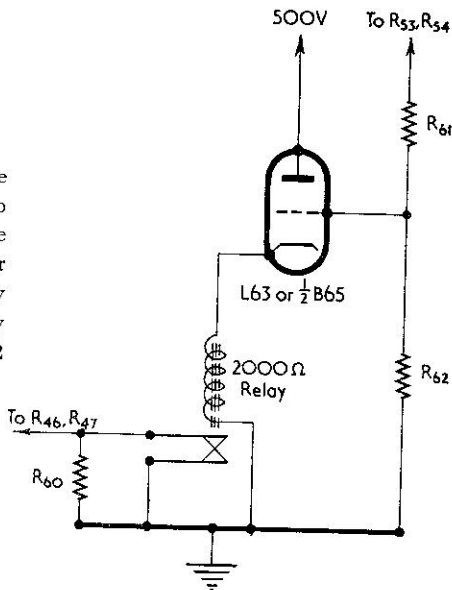


Fig. 7.

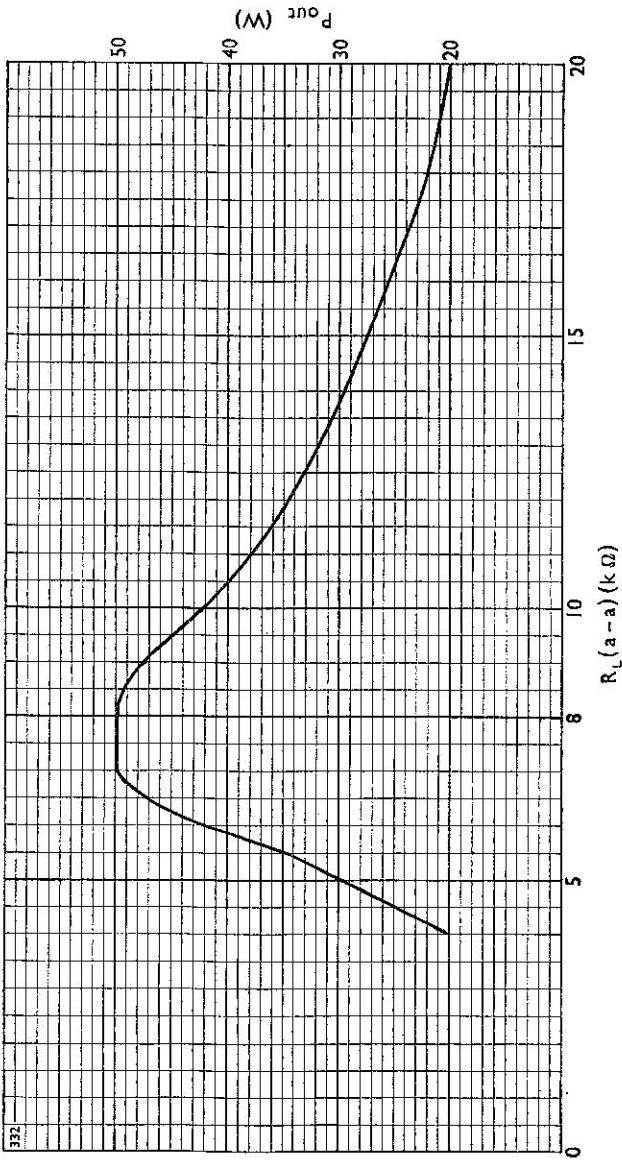


Fig. 8.